Rotor Initial Position Estimation Based on sDFT for Electrically Excited Synchronous Motors

Qing-qing YUAN*, Xiao-jie WU**† and Peng DAI*

*†Dept. of Information and Electronic Engineering, China University of Mining and Technology, Xu Zhou, China

Abstract

Rotor initial position is an important factor affecting the control performance of electrically excited synchronous motors. This study presents a novel method for estimating rotor initial position based on sliding discrete Fourier transform (sDFT). By injecting an ac excitation into the rotor winding, an induced voltage is generated in stator windings. Through this voltage, the stator flux can be obtained using a pure integral voltage model. Considering the influence from a dc bias and an integral initial value, we adopt the sDFT to extract the fundamental flux component. A quadrant identification model is designed to realize the accurate estimation of the rotor initial position. The sDFT and high-pass filter, DFT, are compared in detail, and the contrast between dc excitation and ac injection is determined. Simulation and experimental results verify that this type of novel method can eliminate the influence of dc bias and other adverse factors, as well as provide a basis for the control of motor drives.

Keywords: Electrically excited synchronous motors, Rotor initial position, Sliding discrete Fourier transform, Quadrant identification

I. INTRODUCTION

Electrically excited synchronous motors (EESMs) are widely applied in high-power industrial drives, such as metal rolling, mine hoisting, ship propulsion, and locomotive traction [1–4] because of their high efficiency and adjustable power factor. The stator frequency of EESM is zero (f_s = 0 Hz) at the starting time. An incorrect estimation of the rotor initial position at this time can affect the success of the start-up and influence the accuracy of the flux observing [5–7].

Numerous studies have been conducted to estimate rotor initial position. The traditional method involved injecting dc excitation into the rotor winding while the stator windings were not electrified, followed by the induced voltage and the flux amplitude. The corresponding angle can be obtained by a pure integral voltage model. However, the traditional method has several disadvantages, including: 1) fast attenuation of the induced voltage because of dc excitation; 2) a dc bias and an integral value resulting from a pure integral voltage model; and 3) other factors, such as inverter nonlinearity, dead zone, and high frequency interference [6–8]. The use of ac excitation as a replacement can solve the fast attenuation problem, but the integral initial value and the dc bias error persist. An improved voltage model can only address the issue of initial value.

High-frequency signal injection [9–11], in which filter performance is an important factor that affects position estimation, is another common approach. Compared with discrete Fourier transform (DFT), sliding DFT (sDFT) can extract a signal spectrum with faster arithmetic speed and simpler implementation [12].

This paper presents a novel estimation method for the rotor initial position of EESM. First, an ac excitation is injected into the rotor winding. Second, flux components can be obtained with the induced voltage through a pure integral voltage model. Third, the fundamental flux is extracted along with the rotor initial position as sDFT settles the dc bias and the initial integral value.

The paper is organized as follows: Section 2 summarizes the problems with the traditional method. Section 3 describes the principle of sDFT and its difference from high-pass filter (HPF) and DFT. Section 4 proposes a novel method based on sDFT with ac rather than dc excitation. Simulation and experimental results are shown in Section 5, and conclusions are provided in Section 6.
II. PROBLEMS WITH THE TRADITIONAL METHOD

A sine induced voltage, which is generated in the stator windings, can avoid fast attenuation with an ac excitation injected into the rotor winding of EESM. The stator voltage vector should be perpendicular to the stator flux under ideal conditions. Once dc bias error occurs during the integration, the relationship among the stator-induced voltage, flux, and rotor initial position in the two-phase static coordinates are as follows:

\[ e_{sa} = \pm a \cdot \cos \theta + \beta_{sa} \]
\[ e_{gb} = \pm b \cdot \cos \theta + \beta_{gb} \]

\[ \psi_{sa} = \int e_{sa} dt = \frac{a}{\omega} \sin \theta + \beta_{sa}T \]  
\[ \psi_{gb} = \int e_{gb} dt = \frac{b}{\omega} \sin \theta + \beta_{gb}T \]  
\[ \phi = \arctan \frac{\psi_{gb}}{\psi_{sa}} \]  
where, \( \beta_{sa}, \beta_{gb} \) are unknown dc biases; \( a \) and \( b \) represent the voltage amplitudes; \( \theta \) and \( \omega \) are the angle and angular frequencies of the induced cosine voltage, respectively, with \( T \) denoting the integral cycle; \( \psi_{sa}, \psi_{gb} \) are the flux components resulting from the integral voltage model; and \( \phi \) is the flux angle, which also refers to the rotor initial position.

In an actual system, \( a \gg \beta_{sa}, b \gg \beta_{gb} \); however, a tiny error can result in a large derivation after integration. When \( \theta = \pi, 2\pi, 3\pi \ldots \), the stator flux in \( \alpha \) coordinate is as follows:

\[ \psi_{sa} = \beta_{sa}T_z \]  
where \( T_z \) represents the cycle when the voltage crosses zero.

Similarly, when \( \theta = \pi, 2\pi, 3\pi \ldots \), the stator flux in the \( \beta \) coordinate is shown as

\[ \psi_{gb} = \beta_{gb}T_z \]  

Aside from the dc bias, dead zone and inverter nonlinearity can cause an incorrect estimation of the rotor initial position.

III. PRINCIPLE OF SDFT

A. Basic principle of sDFT

The sDFT is a recursive implementation of the DFT algorithm, which is often used to calculate the spectrum components of a finite-length signal with low computational cost [12–14].

Given a continuous signal in time domain \( x(t) \), the fundamental frequency is \( f_0 \). With discrete sampling (sampling frequency is \( f_s \)), this continuous signal can be transformed into a finite length sequence \( x(n) \), with the length as \( N = f_s/f_0 \). The DFT of \( x(n) \) is

\[ X(k) = \text{DFT}[x(n)] = \sum_{n=0}^{N-1} x(n)W_N^{nk}, (0 \leq k \leq N - 1) \]  
where \( W_N = e^{2\pi i/N} \).

Equation (6) can be expanded as follows:

\[ X(k) = x(0) + x(1)e^{-\frac{2\pi k}{N}} + x(2)e^{-\frac{2\pi k+2}{N}} + \cdots + x(N-1)e^{-\frac{2\pi k(N-1)}{N}} \]  

Equation (7) requires \( N \) data to extract the fundamental component, which adversely influences calculation speed.

Assuming that we have two finite-length sequences \( x_0(n) \) and \( x_1(n) \), the lengths of which are both \( N \), the relationship between \( x_0(n) \) and \( x_1(n) \) is shown in Fig. 1.

![Fig. 1 Data graphics of \( x_0(n) \) and \( x_1(n) \)](image)

The DFTs of the two sequences are \( X_0(k) \) and \( X_1(k) \).

\[ X_0(k) = x(0) + x(1)e^{-\frac{2\pi k}{N}} + x(2)e^{-\frac{2\pi k+2}{N}} + \cdots + x(N-1)e^{-\frac{2\pi k(N-1)}{N}} \]  

\[ X_1(k) = x(1) + x(2)e^{-\frac{2\pi k}{N}} + x(3)e^{-\frac{2\pi k+2}{N}} + \cdots + x(N)e^{-\frac{2\pi k(N-1)}{N}} \]  

Equation (9) indicates that the DFT of \( x_1(n) \) takes new sampled data \( x_1(N+1) \) as a replacement for \( x_0(0) \). Substituting Equation (8) into Equation (9), \( X_1(k) \) can be re-written as

\[ X_1(k) = X_0(k) - x(0) + x(N) \]  

Equation (10) shows that \( X_1(k) \) can calculated only by using the DFT of \( x_0(n) \), that is, \( X_0(k) \), and \( x(0), x(N) \), along with a simple phase-shift computation.

The transfer function of sDFT that extracts \( k \)-harmonic in the z-domain is presented in Equation (11), and its structure is shown in Fig. 2.

\[ H_{sDFT}(z) = \frac{1-z^{-N}e^{j2\pi k/N}}{1-e^{j2\pi k/N}z^{-1}} \]  

![Fig. 2 Implementation structure of sDFT in the z-domain](image)
B. Comparison between DFT and HPF

Sliding DFT and DFT (which can be taken as a main value sequence of DFS) exhibit similar characteristics with the sole difference being implementation speed. The ratio of calculation amount between DFT and sDFT is \((\log_2 N)/2\), provided the same data number \(N\) [12].

HPF, in which cut-off frequency, order, and type crucially impact the filter dynamic response process and the estimation precision, can restrain dc bias along with a simple implementation [15]. For example, a low cut-off frequency is beneficial to improve the estimation accuracy for a 2-order Butterworth HPF. However, the dynamic response slows down because of the large time delay. Thus, although a high cut-off frequency can speed up the dynamic estimation process, such frequency will cause waveform distortion and affect the estimation accuracy.

We assume an input signal \(x_0 = \sin(2\pi f_0 t) + 0.2\), where \(f_0 = 50\) Hz, and 0.2 is the dc bias. The fundamental component of the input signal extracted by sDFT and HPF are compared using MATLAB.

As regards sDFT, the sampling frequency \(f_s = 5\) kHz, and the data number \(N = f_s/f_0 = 400\). The cut-off frequency of HPF is set at different values (\(f_c = 1\) Hz, \(f_c = 10\) Hz, and \(f_c = 20\) Hz). The simulation waveforms are shown in Figs. 3, 4, and 5.

![Fig. 3 Simulation results of sDFT \((N = 400)\) and HPF \((f_c = 1\) Hz)](image)

![Fig. 4 Simulation results of sDFT \((N = 400)\) and HPF \((f_c = 10\) Hz)](image)

![Fig. 5 Simulation results of sDFT \((N = 400)\) and HPF \((f_c = 20\) Hz)](image)

Figs. 3 to 5 illustrate that sDFT and HPF can restrain the dc bias within one fundamental period. However, when \(f_c = 1\) Hz, HPF tracks performance precisely at a steady state with the dynamic adjustment time at nearly six to eight fundamental periods, as shown in Fig. 3. Although increasing \(f_c\) can accelerate the dynamic process, his condition can result in low precision, as shown in Figs. 4 and 5.

In addition, sDFT can extract harmonic or dc bias components any time by setting different \(k\) values in Equation (11). The dc bias in input signal \(x_0\) obtained by sDFT is shown in Fig. 6. When \(x_0 = \sin(2\pi f_0 t) + 0.3\sin(6\pi f_0 t) + 0.2\), the estimation results of sDFT \((N = 400, k = 1)\) and HPF \((f_c = 1\) Hz) are shown in Fig. 7.

![Fig. 6 DC bias obtained by sDFT \((N = 400)\)](image)

![Fig. 7 Simulation results of sDFT \((N = 400, k = 1)\) and HPF \((f_c = 1\) Hz) with a harmonic input)](image)

IV. APPROACH TO ESTIMATE THE ROTOR INITIAL POSITION BASED ON SDFT

The flux obtained from the integral voltage model can be regarded as finite sequences. We define sequences \(\psi_0(n)\), \(\psi_1(n)\) as \(x_0(n)\) and \(x_1(n)\) in Fig. 1, and their DFTs are
\[
\Psi_0(k) = \psi(0) + \psi(1)e^{-\frac{2nk}{N}} + \psi(2)e^{-\frac{2nk+2}{N}} + \ldots
\]
(12)

\[
\Psi_1(k) = [\Psi_0(k) - \psi(0)]e^{-\frac{2nk}{N}} + \psi(N)e^{-\frac{2nk(N-1)}{N}}
\]
(13)

where \(\Psi_0(k)\) and \(\Psi_1(k)\) are complex components. When \(k = 1\), \(\Psi_0(1)\) and \(\Psi_1(1)\) represent the fundamental components, which can be decomposed into the real and imaginary components, through which the fundamental components \(\psi'_{sa}, \psi'_{sb}\) and their amplitudes \(|\psi'_{sa}|, |\psi'_{sb}|\), as well as their angle \(\arctan \psi'_{sa}, \psi'_{sb}\) in the first half of the cycle. Then, the quadrant can be determined according to the flux sign (plus or minus), as well as the identifiers, \(A\) and \(B\). The possible quadrant with different rotor initial positions is shown in Table 1.

**TABLE I**

<table>
<thead>
<tr>
<th>Flux sign (\psi'<em>{sa}, \psi'</em>{sb})</th>
<th>Quadrant</th>
<th>Identifiers</th>
<th>(A), (B)</th>
</tr>
</thead>
<tbody>
<tr>
<td>(\psi'<em>{sa} &gt; 0, \psi'</em>{sb} &gt; 0)</td>
<td>First quadrant</td>
<td>(A = 0, B = 1)</td>
<td></td>
</tr>
<tr>
<td>(\psi'<em>{sa} &lt; 0, \psi'</em>{sb} &gt; 0)</td>
<td>Second quadrant</td>
<td>(A = 1, B = -1)</td>
<td></td>
</tr>
<tr>
<td>(\psi'<em>{sa} &lt; 0, \psi'</em>{sb} &lt; 0)</td>
<td>Third quadrant</td>
<td>(A = -1, B = 1)</td>
<td></td>
</tr>
<tr>
<td>(\psi'<em>{sa} &gt; 0, \psi'</em>{sb} &lt; 0)</td>
<td>Fourth quadrant</td>
<td>(A = 0, B = -1)</td>
<td></td>
</tr>
</tbody>
</table>

The rotor initial position \(\varphi'\) can be calculated by Using Equation (14).

\[
\varphi' = A \cdot \pi + B \cdot \arctan \left( \frac{|\psi'_{sa}|}{|\psi'_{sb}|} \right)
\]
(14)

The detailed implementation for the rotor initial position estimation proposed in this paper is shown in Fig. 8, and the flowchart of the implementation is shown in Fig. 9.

**V. SIMULATION AND EXPERIMENTAL RESULTS**

**A. Simulation results**

A simulation was established in MATLAB. In this simulation, the rotor initial position was set at 60° and the dc bias errors of the induced stator voltage \(u_a\) and \(u_b\) were 0.3 and 0.5 V, respectively. When ac excitation was injected into the rotor winding, the induced voltage in stator windings are shown in Fig. 10(a), whereas the flux in the \(ab\) coordinates obtained through the integral voltage model are presented in Fig. 10(b). The fundamental components of the induced flux calculated by sDFT are shown in Fig. 10(c), whereas their amplitudes are shown in Fig. 10(d). The estimated rotor initial position is presented in Fig. 10(e).
Estimation of the rotor initial position based on sDFT for …

This kind of estimation method can be applied once dc excitation is injected into the rotor winding. Another simulation was established in MATLAB with the same configurations, and the fundamental components of the induced flux calculated by sDFT are shown in Fig. 11(a). The estimated rotor initial position is shown in Fig. 11(b).

B. Experimental results

An experimental platform for a 380 V, 50 kW EESM was established to verify the effectiveness of the proposed estimation method. The experimental structure is shown in Fig. 12, whereas the detailed parameters of EESM are shown in Table 2.

Fig. 12 Circuit block diagram of the rotor initial position estimation with voltage sensors
TABLE 2
DETAILED PARAMETERS OF EESM

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Value</th>
</tr>
</thead>
<tbody>
<tr>
<td>Rated Power</td>
<td>50 kW</td>
</tr>
<tr>
<td>Rated voltage</td>
<td>380 V</td>
</tr>
<tr>
<td>Rated frequency</td>
<td>50 Hz</td>
</tr>
<tr>
<td>Rated speed</td>
<td>1500 rpm</td>
</tr>
<tr>
<td>Rated power factor</td>
<td>0.9</td>
</tr>
<tr>
<td>Rated stator current</td>
<td>84.41 A</td>
</tr>
<tr>
<td>Stator resistance</td>
<td>0.059 Ω</td>
</tr>
<tr>
<td>Direct axis reaction reactance</td>
<td>2.38 pu.</td>
</tr>
<tr>
<td>Quadrature axis reaction reactance</td>
<td>1.22 pu.</td>
</tr>
<tr>
<td>Exciting resistance</td>
<td>9.276 Ω</td>
</tr>
<tr>
<td>Stator leakage reactance</td>
<td>0.121 pu.</td>
</tr>
</tbody>
</table>

Common voltage sensors can induce high-frequency interference and quantization error during the sampling process, which affect estimation accuracy. In this paper, we used an oscilloscope (DPO3014) to monitor the induced voltage in stator windings and calculated real-time data using a digital signal proceeding (DSP) processor. The experimental structure without voltage sensors is shown in Fig. 13.

During the experiment, the peak–peak value of the ac excitation current is 1 A, with a 5Hz frequency and 128 sDFT points. The excitation current and the induced voltage in a-phase are shown in Fig. 14.

Figure 15 shows the fundamental flux $\psi_s^\alpha$ and $\psi_s^\beta$ obtained through sDFT when the real rotor position is 60°. The estimated rotor initial position is shown in Fig. 16 (CH1), and the (CH2) illustrates the zero drift during flux crossing.

Figure 17 shows the experimental results when the real rotor position is horizontal coordinate and the estimated position error is vertical. This presents an estimation error within ±1° as well.
Estimation of the rotor initial position based on sDFT for …

The real process of the estimation method applied for the starting process of EESM is shown in Fig. 18. The estimation section for the rotor initial position occurred when $t = 1$ s to 2 s, and the ac excitation injected into the rotor winding was established during $t = 2s - 5s$. When $t = 5$ s to 7 s was the accelerating process and the machine was maintained at 300 rpm after $t = 7$ s. These experimental results verify the effectiveness of the improved estimation method, which can be applied to the actual drive system.

Fig. 18 Starting process of the EESM

VI. CONCLUSION

This paper presented a novel estimation method for the rotor initial position of EESMs based on sDFT. First, an induced voltage was generated in the stator windings by injecting ac excitation into the rotor winding. Second, the induced stator flux resulted from the integral voltage model, which caused such problems as dc bias and initial value of integration. Third, the fundamental component of the induced flux was obtained through sDFT, with which the rotor initial position was estimated.

This proposed method possessed a simplified structure, easy implementation, strong anti-interference, and minimal hardware consumption. Comparisons between sDFT and HPF, with ac and dc excitations, were conducted. Experimental results verified the effectiveness of the proposed method.

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Qing-qing YUAN was born in NanTong, JiangSu, China in 1987. She received her B.S. and M.S. from the China University of Mining and Technology, China, in 2009 and 2011, respectively. She began her Ph.D. program in 2011 with the Department of Information and Electrical Engineering, China University of Mining and Technology. Her current research interests include the modeling and control of high power drives with a low switching frequency.

Xiao-jie WU was born in HengYang, HuNan, China, in 1966. He received his B.S. in Industrial Automation from the China University of Mining and Technology, China, in 1988, and his M.S. and Ph.D. in Electrical Engineering from the China University of Mining and Technology, China, in 1991 and 2000, respectively. From 2002 to 2004, he conducted postdoctoral research at Tsinghua University, Beijing, China. He has been with the Department of Information and Electrical Engineering, China University of Mining and Technology, China, since 1991, where he is currently a Professor. His current research interests include the stability of ac machines, advanced control of electrical machines, and power electronics.

Peng Dai was born in HuaiBei, AnHui, China, in 1973. He received his B.S. in Electrical Engineering from the AnHui University of Science and Technology, Huainan, China, in 1994, and his M.S. and Ph.D. in Electrical Engineering from the China University of Mining and Technology, China, in 1998 and 2006, respectively. He has been with the Department of Information and Electrical Engineering, China University of Mining and Technology, China, since 1998, where he is currently a Professor. His current research interests include the stability and control of synchronous machines.